

## 500MHz Triple 2:1 Gain-of-2, Multiplexing Amplifier

The ISL59448 is a triple channel 2:1 multiplexer featuring integrated buffers with a fixed gain of 2, high slew-rate and excellent bandwidth for video switching. The device features a three-state output (HIZ), which allows the outputs of multiple devices to be tied together. A power-down mode (ENABLE) is included to turn off un-needed circuitry in power sensitive applications. When the ENABLE pin is pulled high, the part enters a power-down mode and consumes just 14mW. An additional feature is a latch enable function (LE) that allows independent logic control using a common logic bus.

### Ordering Information

PART NUMBER	PACKAGE	TAPE & REEL	PKG. DWG. #
ISL59448IAZ (See Note)	24 Ld QSOP (Pb-free)	-	MDP0040
ISL59448IAZ-T7 (See Note)	24 Ld QSOP (Pb-free)	7"	MDP0040

NOTE: Intersil Pb-free plus anneal products employ special Pb-free material sets; molding compounds/die attach materials and 100% matte tin plate termination finish, which are RoHS compliant and compatible with both SnPb and Pb-free soldering operations. Intersil Pb-free products are MSL classified at Pb-free peak reflow temperatures that meet or exceed the Pb-free requirements of IPC/JEDEC J STD-020.

### Features

- 500MHz bandwidth
- $\pm 1600$  V/ $\mu$ s slew rate
- High impedance buffered inputs
- Internally set gain-of-2
- High speed three-state outputs (HIZ)
- Power-down mode ( $\overline{\text{ENABLE}}$ )
- Latch enable
- $\pm 5$ V operation
- Supply current 11mA/ch
- Pb-free plus anneal available (RoHS compliant)

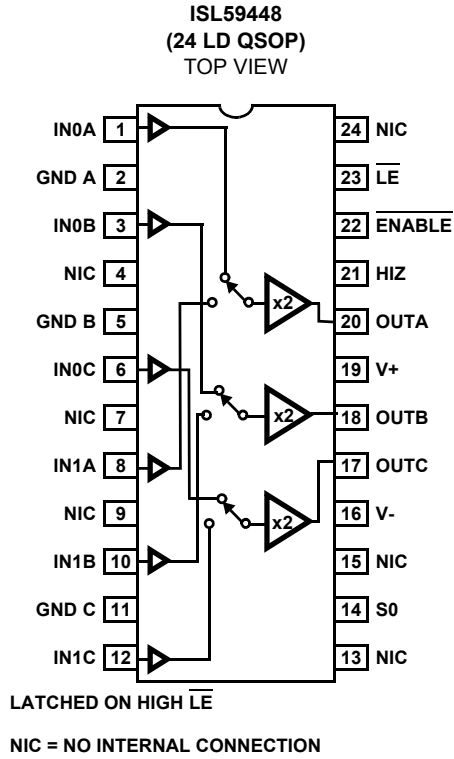
### Applications

- HDTV/DTV analog inputs
- Video projectors
- Computer monitors
- Set-top boxes
- Security video
- Broadcast video equipment

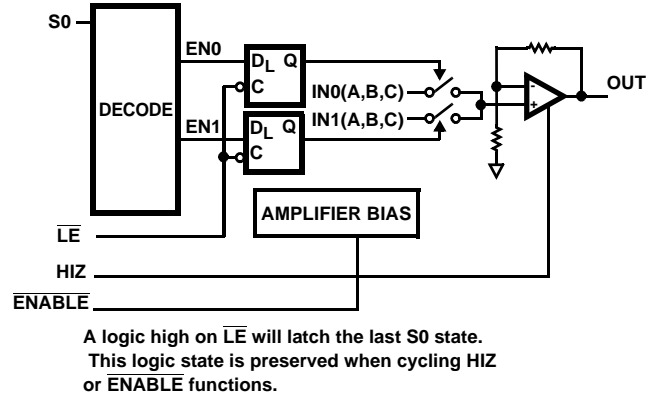
**TABLE 1. CHANNEL SELECT LOGIC TABLE ISL59448**

S0	$\overline{\text{ENABLE}}$	HIZ	$\overline{\text{LE}}$	OUTPUT
0	0	0	0	INO (A, B, C)
1	0	0	0	IN1 (A, B, C)
X	1	X	X	Power-down
X	0	1	X	High Z
X	0	0	1	Last S0 State Preserved

Pinout



Functional Diagram (each channel)



**Absolute Maximum Ratings** ( $T_A = 25^\circ\text{C}$ )

Supply Voltage (V+ to V-)	11V	Storage Temperature Range	-65°C to +150°C
Input Voltage	V- -0.5V, V+ +0.5V	Ambient Operating Temperature	-40°C to +85°C
Supply Turn-on Slew Rate	1V/ $\mu\text{s}$	Operating Junction Temperature	-40°C to +125°C
Digital & Analog Input Current (Note 1)	50mA	Power Dissipation	See Curves
Output Current (Continuous)	50mA		
<b>ESD Rating</b>			
Human Body Model (Per MIL-STD-883 Method 3015.7)	2500V		
Machine Model	300V		

*CAUTION: Stresses above those listed in "Absolute Maximum Ratings" may cause permanent damage to the device. This is a stress only rating and operation of the device at these or any other conditions above those indicated in the operational sections of this specification is not implied.*

**NOTE:**

1. If an input signal is applied before the supplies are powered up, the input current must be limited to these maximum values.

*IMPORTANT NOTE: All parameters having Min/Max specifications are guaranteed. Typical values are for information purposes only. Unless otherwise noted, all tests are at the specified temperature and are pulsed tests, therefore:  $T_J = T_C = T_A$*

**Electrical Specifications** V+ = +5V, V- = -5V, GND = 0V,  $T_A = 25^\circ\text{C}$ ,  $V_{out} = \pm 2V_{P-P}$  &  $R_L = 500\Omega$  to GND,  $C_L = 0\text{pF}$ , unless otherwise specified.

PARAMETER	DESCRIPTION	CONDITIONS	MIN	TYP	MAX	UNIT
<b>GENERAL</b>						
+I <sub>S</sub> Enabled	Enabled Supply Current	No load, V <sub>IN</sub> = 0V, $\overline{\text{Enable}}$ Low	27	31	35	mA
-I <sub>S</sub> Enabled	Enabled Supply Current	No load, V <sub>IN</sub> = 0V, $\overline{\text{Enable}}$ Low	-32	-29	-25	mA
+I <sub>S</sub> Disabled	Disabled Supply Current	No load, V <sub>IN</sub> = 0V, $\overline{\text{Enable}}$ High	2.3	2.7	3.3	mA
-I <sub>S</sub> Disabled	Disabled Supply Current	No load, V <sub>IN</sub> = 0V, $\overline{\text{Enable}}$ High	-0.1		0.1	mA
V <sub>OUT</sub>	Positive and Negative Output Swing	V <sub>IN</sub> = $\pm 2.5V$ ; R <sub>L</sub> = 500 $\Omega$	$\pm 3.1$	$\pm 3.9$		V
I <sub>OUT</sub>	Output Current	V <sub>IN</sub> = 0.825V R <sub>L</sub> = 10 $\Omega$	$\pm 80$		$\pm 180$	mA
V <sub>OS</sub>	Output Offset Voltage		-40	-25	-10	mV
I <sub>b</sub>	Input Bias Current	V <sub>IN</sub> = 0V	-3	-2	-1	$\mu\text{A}$
R <sub>OUT</sub>	HIZ Output Resistance	HIZ = Logic High	700	900	1150	$\Omega$
R <sub>OUT</sub>	Enabled Output Resistance	HIZ = Logic Low		0.2		$\Omega$
R <sub>IN</sub>	Input Resistance	V <sub>IN</sub> = $\pm 1.75V$		10		M $\Omega$
A <sub>CL</sub> or A <sub>V</sub>	Voltage Gain	R <sub>L</sub> = 500 $\Omega$	1.94	1.98	2.035	V/V
<b>LOGIC</b>						
V <sub>IH</sub>	Input High Voltage (Logic Inputs)			2		V
V <sub>IL</sub>	Input Low Voltage (Logic Inputs)			0.8		V
I <sub>IH</sub>	Input High Current (Logic Inputs)	V <sub>H</sub> = 5V	200	258	319	$\mu\text{A}$
I <sub>IL</sub>	Input Low Current (Logic Inputs)	V <sub>L</sub> = 0V	-3		3	$\mu\text{A}$
<b>AC GENERAL</b>						
PSRR	Power Supply Rejection Ratio	DC, PSRR V+ & V- combined V <sub>OUT</sub> = 0dBm	52	72		dB
Xtalk	Channel to Channel Crosstalk	f = 10MHz, ChX-Ch Y-Talk V <sub>IN</sub> = 1V <sub>p-p</sub> ; C <sub>L</sub> = 1.1pF		88		dB
Off - ISO	Off-state Isolation	f = 10MHz, Ch-Ch Off Isolation V <sub>IN</sub> = 1V <sub>p-p</sub> ; C <sub>L</sub> = 1.1pF		72		dB
dG	Differential Gain Error	NTC-7, R <sub>L</sub> = 150, C <sub>L</sub> = 1.1pF		0.015		%
dP	Differential Phase Error	NTC-7, R <sub>L</sub> = 150, C <sub>L</sub> = 1.1pF		0.015		°

# ISL59448

**Electrical Specifications**  $V_+ = +5V$ ,  $V_- = -5V$ ,  $GND = 0V$ ,  $T_A = 25^\circ C$ ,  $V_{out} = \pm 2V_{p-p}$  &  $R_L = 500\Omega$  to  $GND$ ,  $C_L = 0pF$ , unless otherwise specified. **(Continued)**

PARAMETER	DESCRIPTION	CONDITIONS	MIN	TYP	MAX	UNIT
BW	Small Signal -3dB Bandwidth	$V_{OUT} = 0.2V_{p-p}$ ; $R_L = 500\Omega$ , $C_L = 1.1pF$		570		MHz
	Large Signal -3dB Bandwidth	$V_{OUT} = 2V_{p-p}$ ; $R_L = 500\Omega$ , $C_L = 1.1pF$		280		MHz
	Small Signal -3dB Bandwidth	$V_{OUT} = 0.2V_{p-p}$ ; $R_L = 150\Omega$ , $C_L = 1.1pF$		510		MHz
	Large Signal -3dB Bandwidth	$V_{OUT} = 2V_{p-p}$ ; $R_L = 150\Omega$ , $C_L = 1.1pF$		260		MHz
FBW	0.1dB Bandwidth	$V_{OUT} = 2V_{p-p}$ ; $R_L = 500\Omega$ , $C_L = 1.1pF$		140		MHz
	0.1dB Bandwidth	$V_{OUT} = 2V_{p-p}$ ; $R_L = 150\Omega$ , $C_L = 1.1pF$		60		MHz
SR	Slew Rate	25% to 75%, $R_L = 150\Omega$ , Input Enabled, $C_L = 1.1pF$		1600		V/ $\mu s$
<b>TRANSIENT RESPONSE</b>						
tr, tf Large Signal	Large Signal Rise, Fall Times, tr, tf, 10% - 90%	$V_{OUT} = 2V_{p-p}$ ; $R_L = 500\Omega$ , $C_L = 1.1pF$		1.2		ns
		$V_{OUT} = 2V_{p-p}$ ; $R_L = 150\Omega$ , $C_L = 1.1pF$		1.3		ns
tr, tf, Small Signal	Small Signal Rise, Fall Times, tr, tf, 10% - 90%	$V_{OUT} = 0.2V_{p-p}$ ; $R_L = 500\Omega$ , $C_L = 1.1pF$		0.7		ns
		$V_{OUT} = 0.2V_{p-p}$ ; $R_L = 150\Omega$ , $C_L = 1.1pF$		0.85		ns
ts 0.1%	Settling Time 0.1%	$V_{OUT} = 2V_{p-p}$ ; $R_L = 500\Omega$ , $C_L = 1.1pF$		5		ns
		$V_{OUT} = 2V_{p-p}$ ; $R_L = 150\Omega$ , $C_L = 1.1pF$		4.5		ns
ts 1%	Settling Time 1%	$V_{OUT} = 2V_{p-p}$ ; $R_L = 500\Omega$ , $C_L = 1.1pF$		2		ns
		$V_{OUT} = 2V_{p-p}$ ; $R_L = 150\Omega$ , $C_L = 1.1pF$		2.5		ns
<b>SWITCHING CHARACTERISTICS</b>						
V <sub>GLITCH</sub>	Channel -to-Channel Switching Glitch	$V_{IN} = 0V$ , $C_L = 1.1pF$		40		mV <sub>p-p</sub>
	Enable Switching Glitch	$V_{IN} = 0V$ , $C_L = 1.1pF$		250		mV <sub>p-p</sub>
	HIZ Switching Glitch	$V_{IN} = 0V$ , $C_L = 1.1pF$		200		mV <sub>p-p</sub>
t <sub>SW-L-H</sub>	Channel Switching Time Low to High	1.2V logic threshold to 10% movement of analog output		18		ns
t <sub>SW-H-L</sub>	Channel Switching Time High to Low	1.2V logic threshold to 10% movement of analog output		20		ns
tpd	Propagation Delay	10% to 10%		0.9		ns
t <sub>LH</sub>	Latch Enable Hold time	$\overline{LE} = 0$		10		ns

**Typical Performance Curves**  $V_S = \pm 5V$ ,  $R_L = 500\Omega$  to GND,  $T_A = 25^\circ C$ , unless otherwise specified.

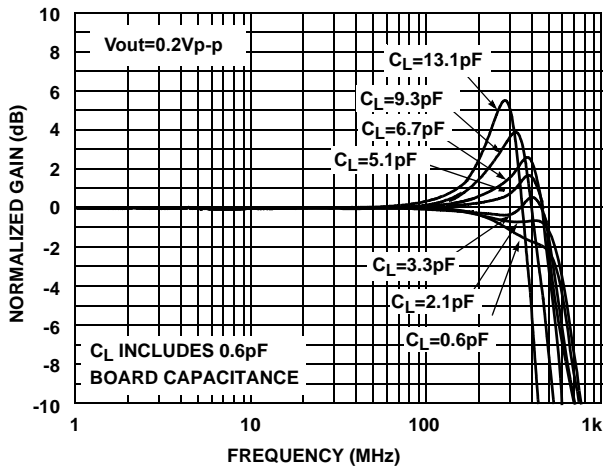


FIGURE 1. SMALL SIGNAL GAIN vs FREQUENCY vs  $C_L$  INTO  $500\Omega$  LOAD

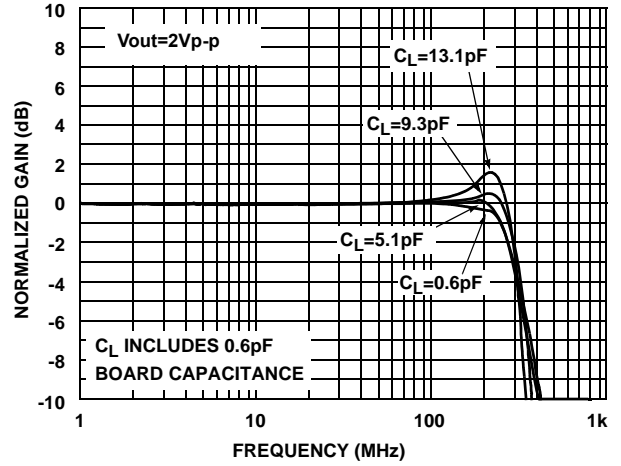


FIGURE 2. LARGE SIGNAL GAIN vs FREQUENCY vs  $C_L$  INTO  $500\Omega$  LOAD

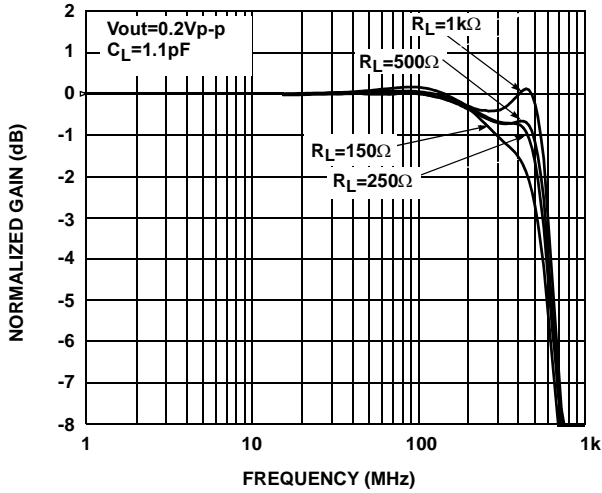


FIGURE 3. GAIN vs FREQUENCY vs  $R_L$

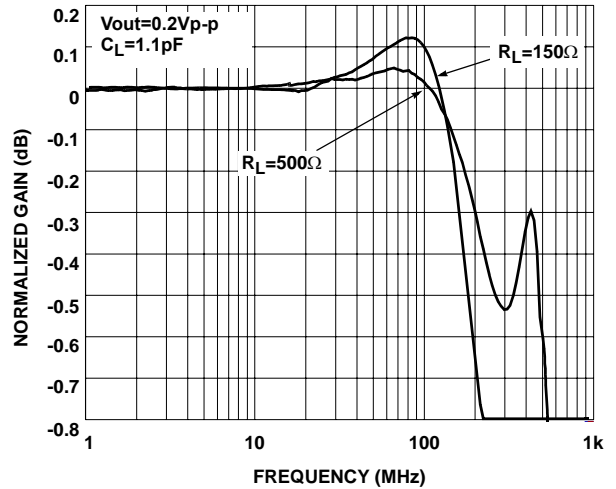


FIGURE 4. 0.1dB GAIN FLATNESS

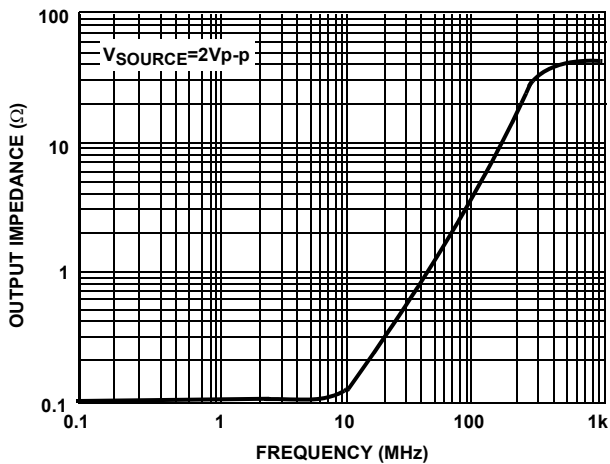


FIGURE 5.  $Z_{OUT}$  vs FREQUENCY - ENABLED

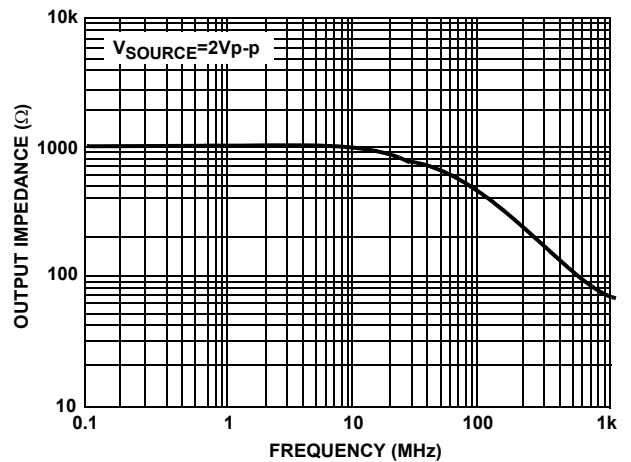


FIGURE 6.  $Z_{OUT}$  vs FREQUENCY - HiZ

**Typical Performance Curves**  $V_S = \pm 5V$ ,  $R_L = 500\Omega$  to GND,  $T_A = 25^\circ C$ , unless otherwise specified. (Continued)

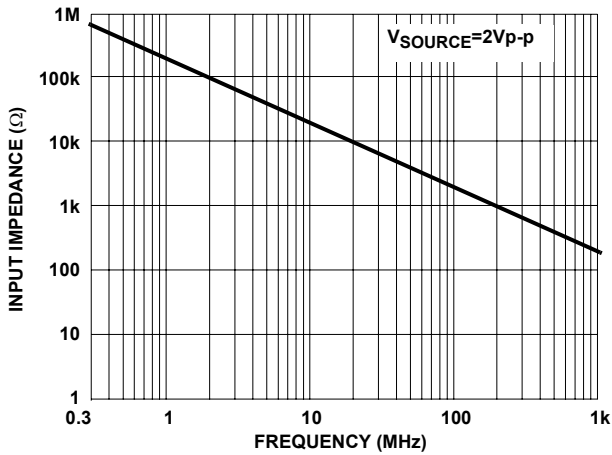


FIGURE 7.  $Z_{IN}$  vs FREQUENCY

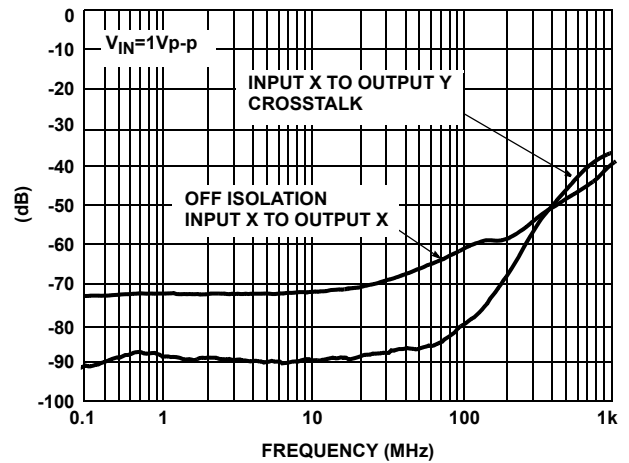


FIGURE 8. CROSSTALK AND OFF-ISOLATION

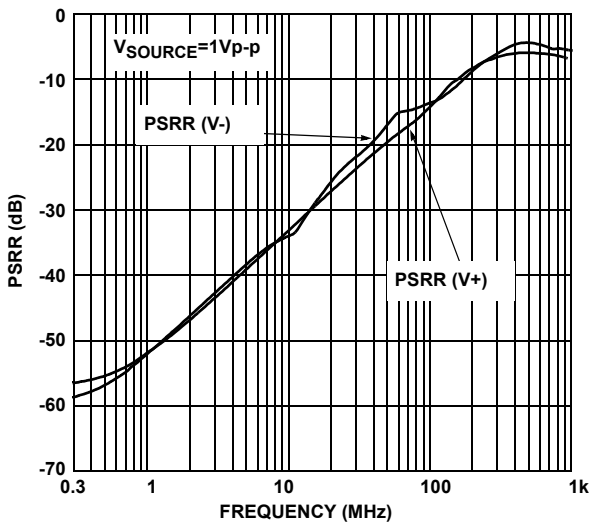


FIGURE 9. PSRR

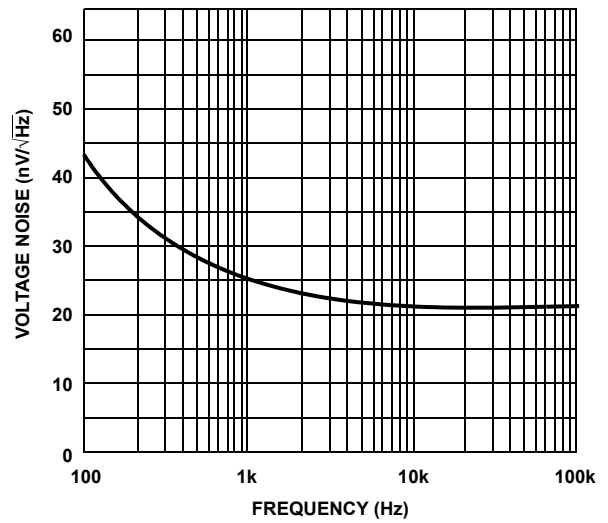


FIGURE 10. INPUT NOISE vs FREQUENCY

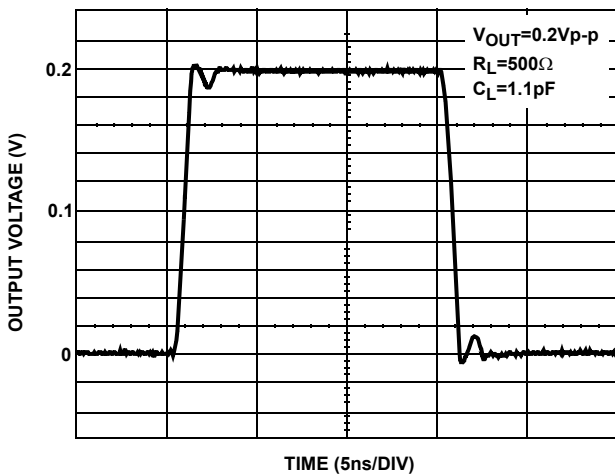


FIGURE 11. SMALL SIGNAL TRANSIENT RESPONSE;  $R_L=500\Omega$

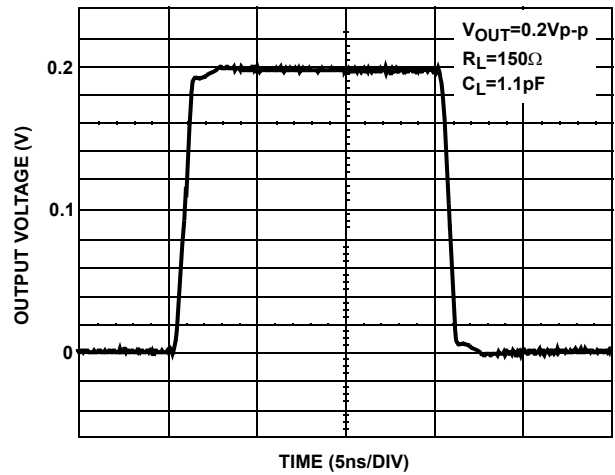


FIGURE 12. SMALL SIGNAL TRANSIENT RESPONSE;  $R_L=150\Omega$

**Typical Performance Curves**  $V_S = \pm 5V$ ,  $R_L = 500\Omega$  to GND,  $T_A = 25^\circ C$ , unless otherwise specified. (Continued)

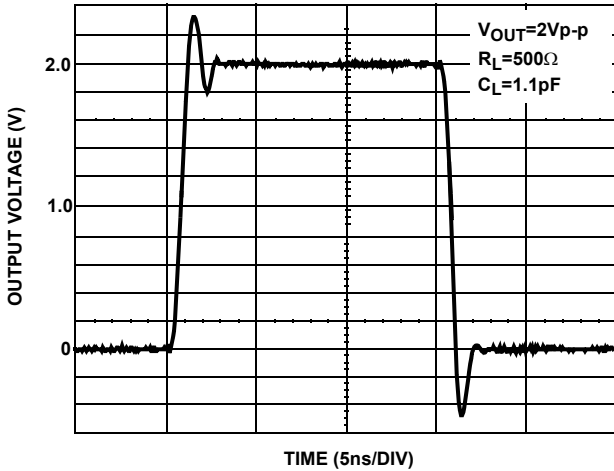


FIGURE 13. LARGE SIGNAL TRANSIENT RESPONSE;  
 $R_L=500\Omega$

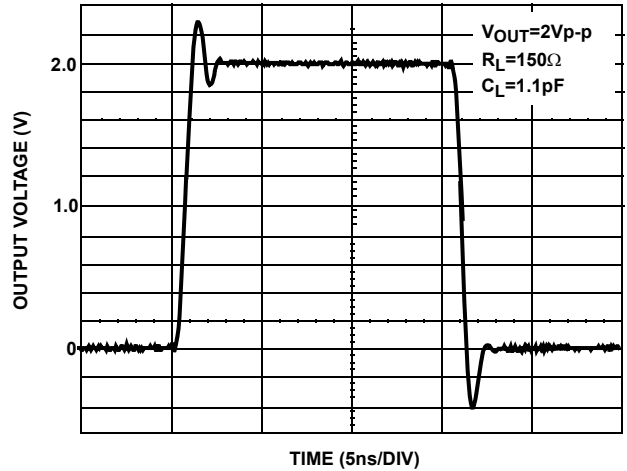


FIGURE 14. LARGE SIGNAL TRANSIENT RESPONSE;  
 $R_L=150\Omega$

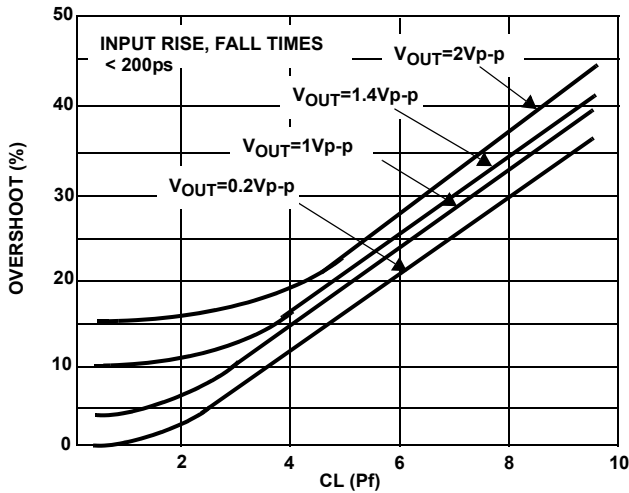


FIGURE 15. POSITIVE PULSE OVERSHOOT vs  $V_{OUT}$ ,  $C_L$ ;  
 $R_L=500\Omega$

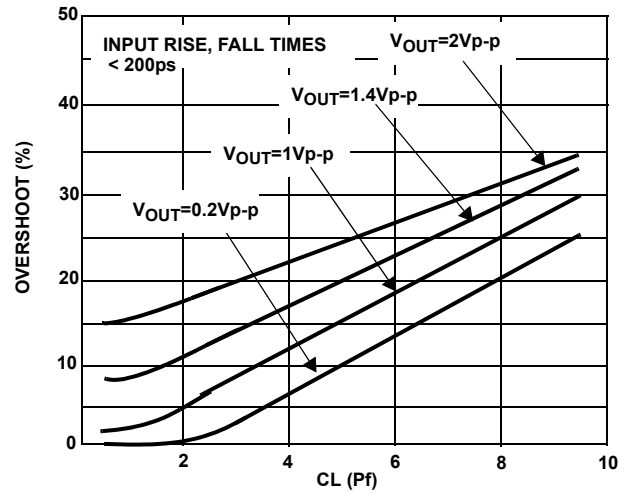


FIGURE 16. POSITIVE PULSE OVERSHOOT vs  $V_{OUT}$ ,  $C_L$ ;  
 $R_L=150\Omega$

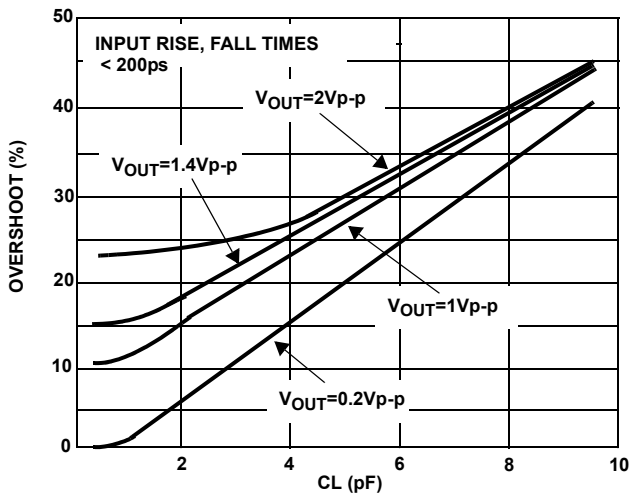


FIGURE 17. NEGATIVE PULSE OVERSHOOT vs  $V_{OUT}$ ,  $C_L$ ;  
 $R_L=500\Omega$

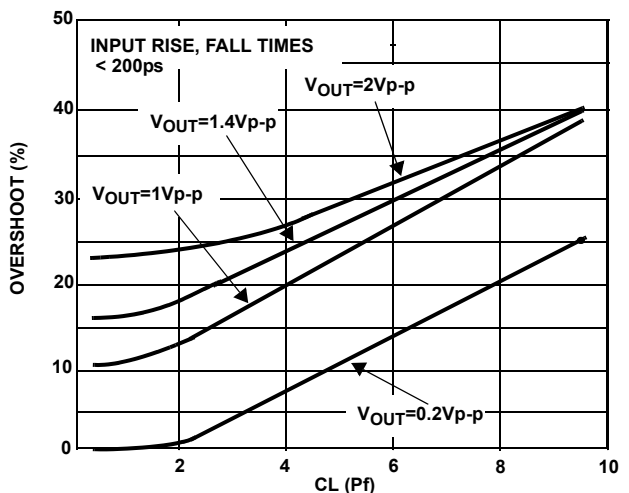


FIGURE 18. NEGATIVE PULSE OVERSHOOT vs  $V_{OUT}$ ,  $C_L$ ;  
 $R_L=150\Omega$

**Typical Performance Curves**  $V_S = \pm 5V$ ,  $R_L = 500\Omega$  to GND,  $T_A = 25^\circ C$ , unless otherwise specified. (Continued)

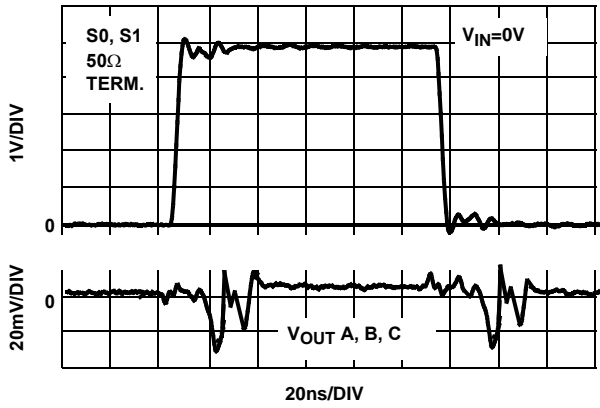


FIGURE 19. CHANNEL TO CHANNEL SWITCHING GLITCH  $V_{IN} = 0V$

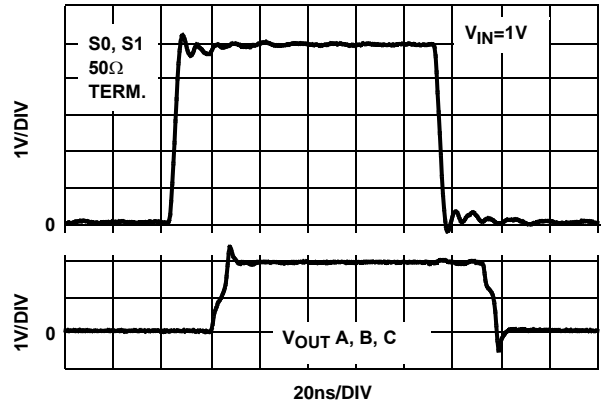


FIGURE 20. CHANNEL TO CHANNEL TRANSIENT RESPONSE  $V_{IN} = 1V$

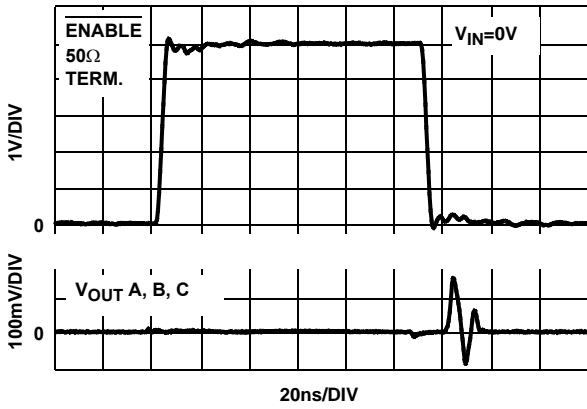


FIGURE 21.  $\overline{\text{ENABLE}}$  SWITCHING GLITCH  $V_{IN} = 0V$

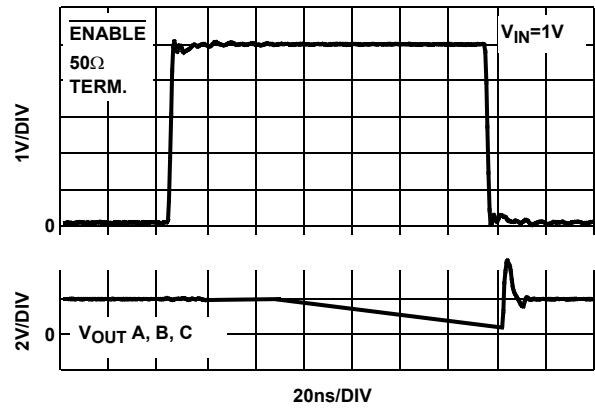


FIGURE 22.  $\overline{\text{ENABLE}}$  TRANSIENT RESPONSE  $V_{IN} = 1V$

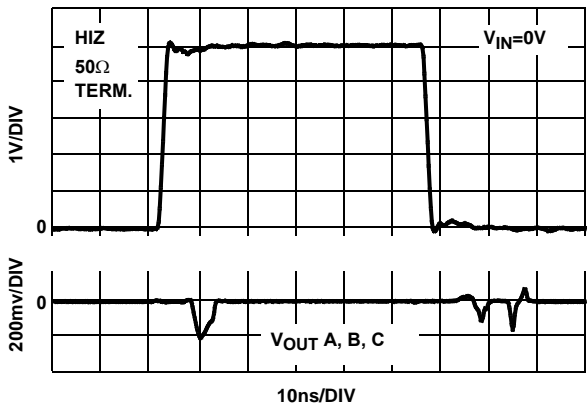


FIGURE 23. HIZ SWITCHING GLITCH  $V_{IN} = 0V$

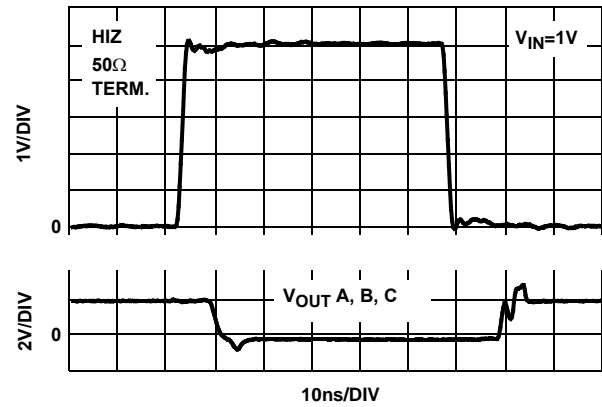


FIGURE 24. HIZ TRANSIENT RESPONSE  $V_{IN} = 1V$



**Typical Performance Curves**  $V_S = \pm 5V$ ,  $R_L = 500\Omega$  to GND,  $T_A = 25^\circ C$ , unless otherwise specified. (Continued)

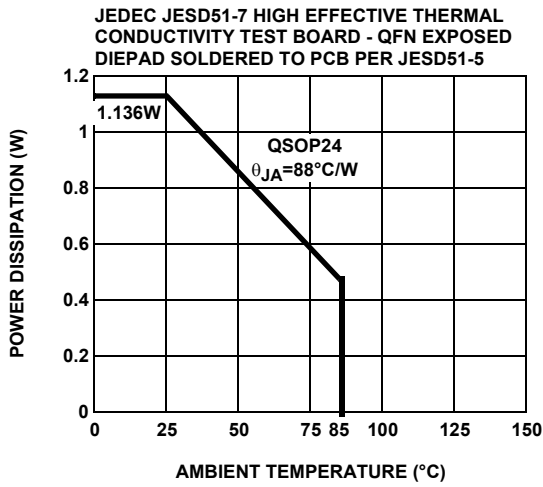


FIGURE 25. PACKAGE POWER DISSIPATION vs AMBIENT TEMPERATURE

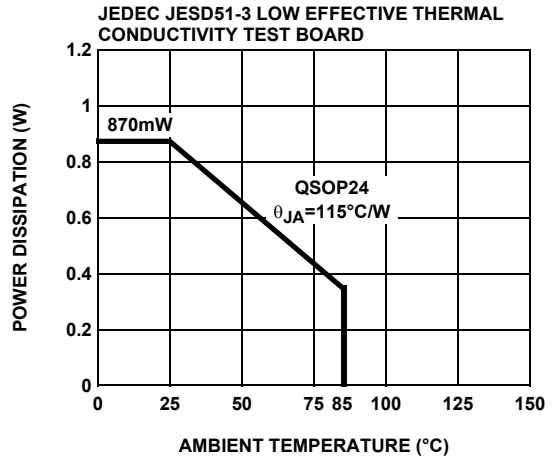
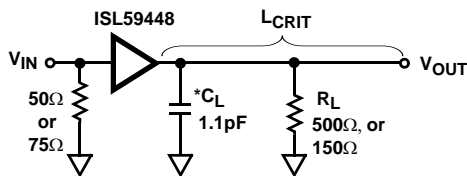


FIGURE 26. PACKAGE POWER DISSIPATION vs AMBIENT TEMPERATURE

**Pin Descriptions**

ISL59448 (24 LD QSOP)	PIN NAME	EQUIVALENT CIRCUIT	DESCRIPTION
8	IN1A	Circuit 1	Channel 1 input for output amplifier "A"
4, 7, 9, 13, 15, 24	NIC		<b>Not Internally Connected</b> ; it is recommended these pins be tied to ground to minimize crosstalk.
10	IN1B	Circuit 1	Channel 1 input for output amplifier "B"
12	IN1C	Circuit 1	Channel 1 input for output amplifier "C"
5	GNDB	Circuit 4	Ground pin for output amplifier "B"
11	GNDC	Circuit 4	Ground pin for output amplifier "C"
14	S0	Circuit 2	Channel selection pin. LSB (binary logic code)
17	OUTC	Circuit 3	Output of amplifier "C"
18	OUTB	Circuit 3	Output of amplifier "B"
16	V-	Circuit 4	Negative power supply
20	OUTA	Circuit 3	Output of amplifier "A"
19	V+	Circuit 4	Positive power supply
22	$\overline{\text{ENABLE}}$	Circuit 2	Device enable (active low) w/Internal pull-down resistor. A logic High puts device into power-down mode with the only logic circuitry active. All logic states are preserved post power-down. This state is not recommended for logic control where more than one MUX-amp share the same video output line.
23	$\overline{\text{LE}}$	Circuit 2	Device latch enable on the ISL59424. A logic high on $\overline{\text{LE}}$ will latch the last (S0, S1) logic state. HIZ and $\overline{\text{ENABLE}}$ functions are not latched with the $\overline{\text{LE}}$ pin.
21	HIZ	Circuit 2	Output disable (active high) w/internal pull-down resistor. A logic high, puts the outputs in a high impedance state. Use this state to control logic when more than one MUX-amp share the same video output line.
6	IN0C	Circuit 1	Channel 0 for output amplifier "C"
3	IN0B	Circuit 1	Channel 0 for output amplifier "B"
1	IN0A	Circuit 1	Channel 0 for output amplifier "A"
2	GNDA	Circuit 4	Ground pin for output amplifier "A"

## AC Test Circuits



\* $C_L$  Includes PCB trace capacitance

FIGURE 27A. TEST CIRCUIT WITH OPTIMAL OUTPUT LOAD

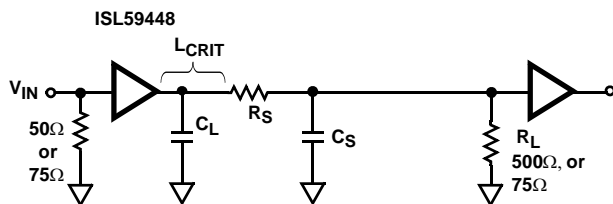
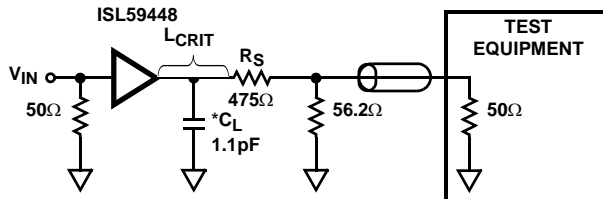
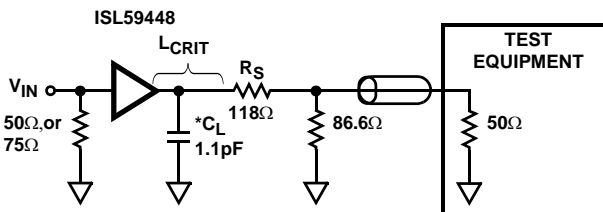


FIGURE 27B. INTER-STAGE APPLICATION CIRCUIT



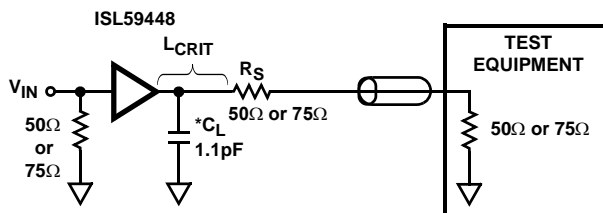
\* $C_L$  Includes PCB trace capacitance

FIGURE 27C. 500Ω TEST CIRCUIT WITH 50Ω LOAD



\* $C_L$  Includes PCB trace capacitance

FIGURE 27D. 150Ω TEST CIRCUIT WITH 50Ω LOAD



\* $C_L$  Includes PCB trace capacitance

FIGURE 27E. BACKLOADED TEST CIRCUIT FOR 75Ω VIDEO CABLE APPLICATION

## AC Test Circuits

Figure 27C and 27D illustrate the optimum output load for testing AC performance at 500Ω and 150Ω loads. Figure 27E illustrates the optimum output load for 50Ω and 75Ω cable-driving.

## Application Information

### General

Key features of the ISL59448 include a fixed gain of 2, buffered high impedance analog inputs and excellent AC performance at output loads down to 150Ω for video cable-driving. The current feedback output amplifiers are stable operating into capacitive loads.

For the best isolation and crosstalk rejection, all GND pins and NIC pins must connect to the GND plane.

### AC Design Considerations

High speed current-feed amplifiers are sensitive to capacitance at the inverting input and output terminals. The ISL59448 has an internally set gain of 2, so the inverting input is not accessible. Capacitance at the output terminal increases gain peaking (Figure 1) and pulse overshoot (Figures 15 thru 18). The AC response of the ISL59448 is optimized for a total capacitance of 1.1pF over the load range of 150Ω to 500Ω.

PC board trace length should be kept to a minimum in order to minimize output capacitance and prevent the need for controlled impedance lines. At 500MHz trace lengths approaching 1" begin exhibiting transmission line behavior and may cause excessive ringing if controlled impedance traces are not used. Figure 27A shows the optimum inter-stage circuit when the total output trace length is less than the critical length of the highest signal frequency.

For applications where pulse response is critical and where inter-stage distances exceed  $L_{CRIT}$ , the circuit shown in Figure 27B is recommended. Resistor  $R_S$  constrains the capacitance seen by the amplifier output to the trace capacitance from the output pin to the resistor. Therefore,  $R_S$  should be placed as close to the ISL59448 output pin as possible. For inter-stage distances much greater than  $L_{CRIT}$ , the back-loaded circuit shown in Figure 27E should be used with controlled impedance PCB lines, with  $R_S$  and  $R_L$  equal to the controlled impedance.

For applications where inter-stage distances are long, but pulse response is not critical, capacitor  $C_S$  can be added to low values of  $R_S$  to form a low-pass filter to dampen pulse overshoot. This approach avoids the need for the large gain correction required by the -6dB attenuation of the back-loaded controlled impedance interconnect. Load resistor  $R_L$  is still required but can be 500Ω or greater, resulting in a much smaller attenuation factor.

### Control Signals

$S_0$ ,  $S_1$ ,  $\overline{ENABLE}$ ,  $\overline{LE}$ ,  $HIZ$  - These are binary coded, TTL/CMOS compatible control inputs. The  $S_0$ ,  $S_1$  pins select the inputs. All three amplifiers are switched simultaneously from their respective inputs. The  $\overline{ENABLE}$ ,  $\overline{LE}$ ,  $HIZ$  pins are used to disable the part to save power, latch in the last logic state and three-state the output amplifiers, respectively. For

control signal rise and fall times less than 10ns the use of termination resistors close to the part will minimize transients coupled to the output.

### Power-up Considerations

The ESD protection circuits use internal diodes from all pins the V+ and V- supplies. In addition, a dV/dT- triggered clamp is connected between the V+ and V- pins, as shown in the Equivalent Circuits 1 through 4 section of the Pin Description table. The dV/dT triggered clamp imposes a maximum supply turn-on slew rate of 1V/μs. Damaging currents can flow for power supply rates-of-rise in excess of 1V/μs, such as during hot plugging. Under these conditions, additional methods should be employed to ensure the rate of rise is not exceeded.

Consideration must be given to the order in which power is applied to the V+ and V- pins, as well as analog and logic input pins. Schottky diodes (Motorola MBR0550T or equivalent) connected from V+ to ground and V- to ground (Figure 4) will shunt damaging currents away from the internal V+ and V- ESD diodes in the event that the V+ supply is applied to the device before the V- supply.

If positive voltages are applied to the logic or analog video input pins before V+ is applied, current will flow through the internal ESD diodes to the V+ pin. The presence of large decoupling capacitors and the loading effect of other circuits connected to V+, can result in damaging currents through the ESD diodes and other active circuits within the device. Therefore, adequate current limiting on the digital and analog inputs is needed to prevent damage during the time the voltages on these inputs are more positive than V+.

### HIZ State

An internal pull-down resistor ensures the device will be active with no connection to the HIZ pin. The HIZ state is established within approximately 15ns (Figure 14) by placing a logic high (>2V) on the HIZ pin. If the HIZ state is selected, the output impedance is ~1000Ω (Figure 6). The supply current during this state is same as the active state.

### ENABLE and Power-down States

The enable pin is active low. An internal pull-down resistor ensures the device will be active with no connection to the ENABLE pin. The Power-down state is established within approximately 200ns (Figure 22), if a logic high (>2V) is placed on the ENABLE pin. In the power-down state, the output has no leakage but has a large variable capacitance (on the order of 15pF), and is capable of being back-driven. Under this condition, large incoming slew rates can cause fault currents of tens of mA. Therefore, the parallel connection of multiple outputs is not recommended unless the application can tolerate the limited powerdown output impedance.

### LE State

The ISL59448 is equipped with a Latch Enable pin. A logic high (>2V) on the LE pin latches the last logic state. This logic state is preserved when cycling HIZ or ENABLE functions.

### Limiting the Output Current

No output short circuit current limit exists on these parts. All applications need to limit the output current to less than 50mA. Adequate thermal heat sinking of the parts is also required.

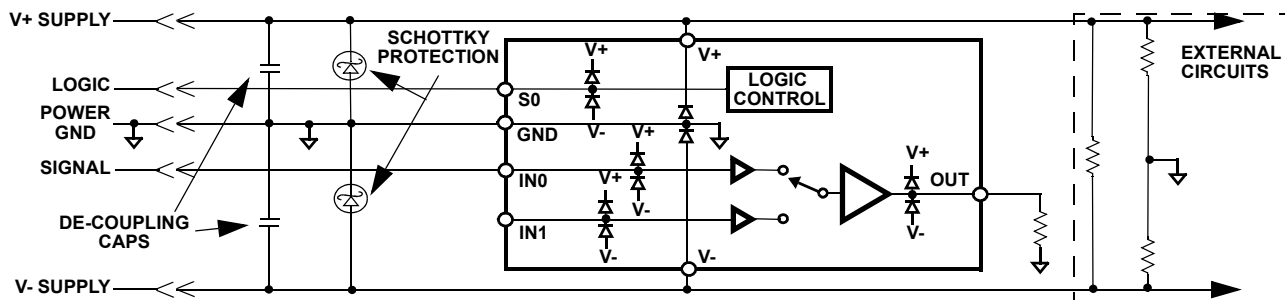


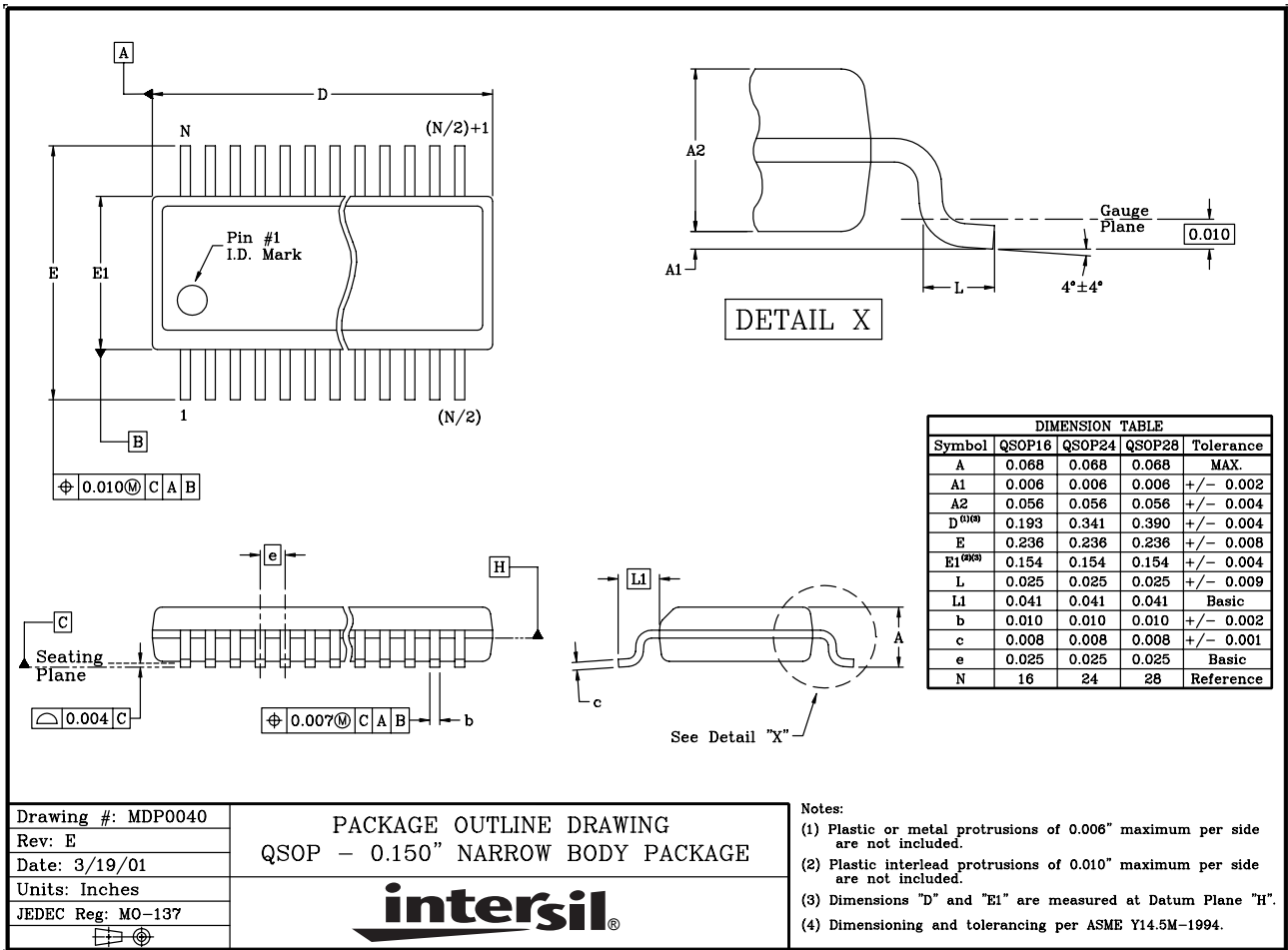
FIGURE 28. SCHOTTKY PROTECTION CIRCUIT

## ***PC Board Layout***

The AC performance of this circuit depends greatly on the care taken in designing the PC board. The following are recommendations to achieve optimum high frequency performance from your PC board.

- The use of low inductance components such as chip resistors and chip capacitors is strongly recommended.
- Minimize signal trace lengths. Trace inductance and capacitance can easily limit circuit performance. Avoid sharp corners, use rounded corners when possible. Vias in the signal lines add inductance at high frequency and should be avoided. PCB traces greater than 1" begin to exhibit transmission line characteristics with signal rise/fall times of 1ns or less. High frequency performance may be degraded for traces greater than one inch, unless strip line are used.
- Match channel-channel analog I/O trace lengths and layout symmetry. This will minimize propagation delay mismatches.
- Maximize use of AC de-coupled PCB layers. All signal I/O lines should be routed over continuous ground planes (i.e. no split planes or PCB gaps under these lines). Avoid vias in the signal I/O lines.
- Use proper value and location of termination resistors. Termination resistors should be as close to the device as possible.
- When testing use good quality connectors and cables, matching cable types and keeping cable lengths to a minimum.
- Minimum of 2 power supply de-coupling capacitors are recommended (1000pF, 0.01 $\mu$ F) as close to the devices as possible - Avoid vias between the cap and the device because vias add unwanted inductance. Larger caps can be farther away. When vias are required in a layout, they should be routed as far away from the device as possible.
- The NIC pins are placed on both sides of the input pins. These pins are not internally connected to the die. It is recommended these pins be tied to ground to minimize crosstalk.

QSOP Package Outline Drawing



NOTE: The package drawing shown here may not be the latest version. To check the latest revision, please refer to the Intersil website at <http://www.intersil.com/design/packages/index.asp>

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